

## Electrically Induced Damage to Standard Linear Integrated Circuits: The Most Common Causes and the Associated Fixes to Prevent Reoccurrence

by Niall Lyne

### INTRODUCTION

The sensitivity of electronic components to transient electrical overstress events is a well-known problem, exacerbated by the continuing evolution of integrated circuits. Smaller geometries, increased circuit densities, and the limited area allotted to on-chip protection all tend to increase this sensitivity. In an effort to minimize costs in each particular segment of system implementation, the burden of transient protection is often shifted to other, less efficient means.

Techniques for protection from “zapping” depend on the stage of manufacture. During the manufacturing of integrated circuits and assembly of electronic equipment, protection is achieved through the use of well-known measures such as static dissipative table tops, wrist straps, ionized air blowers, antistatic shipping tubes, etc. These methods will be discussed only briefly here in relation to Electrostatic Discharge (ESD) protection. Likewise this application note is not addressed to precautionary measures employed during shipping, installation, or repair of equipment. Rather, the main thrust will be limited to protection aspects called upon during printed circuit board assembly, normal operation of the equipment (often by operating personnel who are untrained in preventative measures), and in service conditions where the transient environment may not be well characterized.

The transient environment varies widely. There are substantial differences among those experienced by, say, automotive systems, airborne or shipborne equipment, space systems, industrial equipment or consumer products. All types of electronic components can be destroyed or degraded.<sup>1</sup> Even capacitors, relays, connectors, printed circuit boards, etc., are susceptible, although their threshold levels are much higher than integrated circuits. Microwave diodes and transistors are among the most sensitive components. However, this application note will be restricted to standard linear integrated circuits because of their wide usage, and to limit the scope of coverage.

This application note will first review the nature of the threat to integrated circuits in an operating environment, and then briefly discuss overall device protection from the following: (1) *ESD* events caused by human handling, automatic board insertion equipment, etc., (2) *LATCH-UP* generated from power-up/down sequencing errors, floating ground(s) due to a loose edge connectors, etc., and finally, (3) *HIGH VOLTAGE TRANSIENTS* generated from a power supply, a defective circuit board, during circuit board troubleshooting, etc.

### Electrostatic Discharge

Electrostatic discharge is a single, fast, high current transfer of electrostatic charge that results from:

- Direct contact transfer between two objects at different potentials, *or*
- A high electrostatic field between two objects when they are in close proximity.

The prime sources of static electricity are mostly insulators and are typically synthetic materials, e.g., vinyl or plastic work surfaces, insulated shoes, finished wood chairs, Scotch tape, bubble pack, soldering irons with ungrounded tips, etc. Voltage levels generated by these sources can be extremely high since their charge is not readily distributed over their surfaces or conducted to other objects.

The generation of static electricity caused by rubbing two substances together is called the triboelectric effect. Examples of sources of triboelectric electrostatic charge generation in a high RH ( $\approx 60\%$ ) environment include:

- Walking across a carpet  $\Rightarrow$  1000 V–1500 V generated.
- Walking across a vinyl floor  $\Rightarrow$  150 V–250 V generated.
- Handling material protected by clear plastic covers  $\Rightarrow$  400 V–600 V generated.
- Handling polyethylene bags  $\Rightarrow$  1000 V–1200 V generated.
- Pouring polyurethane foam into a box  $\Rightarrow$  1200 V–1500 V generated.

- ICs sliding down an open antistatic shipping tube  $\Rightarrow$  25 V–250 V generated.

Note: For low RH (<30%) environments, generated voltages can be  $>10 \times$  those listed above.

### ESD Models

To evaluate the susceptibility of devices to simulated stress environments a host of test waveforms have been developed. The three most prominent of these waveforms currently in general use for simulating ESD events in semiconductor or discrete devices are: The Human Body Model (HBM), the Machine Model (MM), and the Charged Device Model (CDM). The test circuits and current waveform characteristics for these three models are shown in Figures 1 to 3. Each of these models represents a fundamentally different ESD event. Consequently, correlation between the test results for these models is minimal.

#### Human Body Model:<sup>2</sup>

Simulates the discharge event that occurs when a person charged to either a positive or negative potential touches an IC at a different potential.

$RLC = 1.5 \text{ k}\Omega, \sim 0 \text{ nH}, 100 \text{ pF}$ .

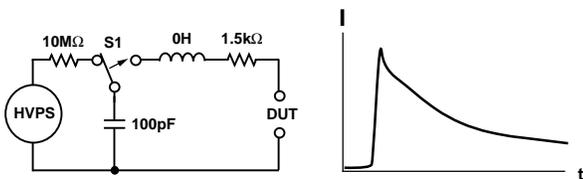


Figure 1. Human Body Model

#### Machine Model:

Japanese model based on a worst-case HBM.

$RLC = 0 \Omega, 500 \text{ nH}, 200 \text{ pF}$ .

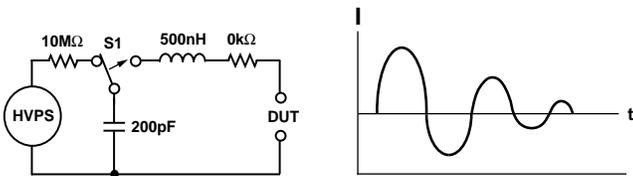


Figure 2. Machine Model

#### Charged Device Model:

Simulates the discharge that occurs when a pin on an IC charged to either a positive or negative potential contacts a conductive surface at a different (usually ground) potential.

$RLC = 0 \Omega, \sim 0 \text{ nH}, 1 \text{ pF} - 20 \text{ pF}$ .

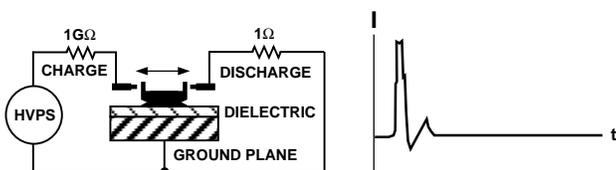


Figure 3. Charged Device Model

### Comparison of HBM, MM, and CDM Waveforms

Figure 4 shows 400 V HBM, MM, and CDM discharge waveforms on the same current vs. time scale. These waveforms are of great use in predicting what failure mechanism may result on a particular device type due to ESD events simulated by one of these three models.

The rise time for the HBM waveform is  $<10 \text{ ns}$  (typically 6 ns–9 ns), and this waveform decays exponentially towards 0 V with a fall time of  $>150 \text{ ns}$ . MIL-STD-883<sup>3</sup> Method 3015 *Electrostatic Discharge Sensitivity Classification* requires a rise time of  $<10 \text{ ns}$  and a delay time of  $150 \pm 20 \text{ ns}$  (Method 3015 defines delay time as the time for the waveform to drop from 90% of the peak current to 36.8% of the peak current). The peak current for the HBM waveform is  $\approx 400 \text{ V}/1500 \Omega$  or 0.267A. Although this peak current is much lower than that for 400 V CDM and MM events, the relatively long duration of the total HBM event results in a discharge of relatively high energy.

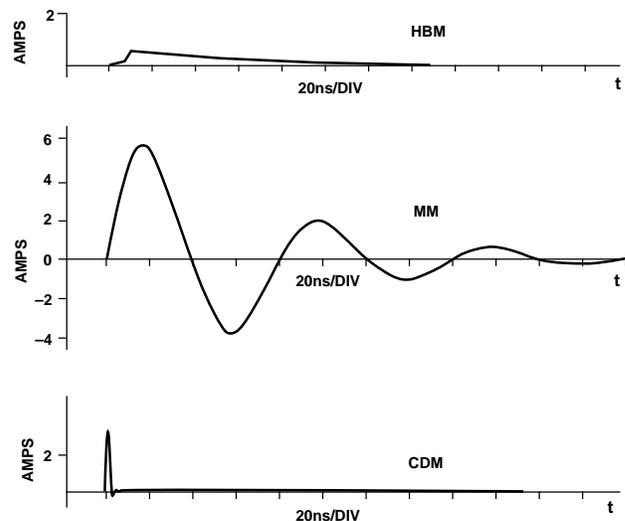


Figure 4. Relative Comparison of 400 V HBM, MM, and CDM Discharges

The MM waveform consists of both positive-going and negative-going sinusoidal peaks with peak magnitudes that decay exponentially. The initial MM peak has a rise time of  $\approx 14 \text{ ns}$ , i.e., only slightly greater than that of the single HBM peak. The total duration of the MM waveform is comparable to that for the HBM waveform. However, the peak current for the first peak of the 400 V MM event is  $\approx 5.8 \text{ A}$ , which is the highest of the three models. The next four peaks, though decreasing in current, still all have magnitudes of  $>1 \text{ A}$ . These multiple high current peaks of substantial duration result in an overall discharge energy that is by far the highest of the three models because there is no current limiting;  $R = 0 \Omega$ .

The CDM waveform corresponds to the shortest known real-world ESD event. The socketed CDM waveform has a rise time of 400 ps, with the total duration of the CDM event of  $\approx 2 \text{ ns}$ . The CDM waveform is essentially unipolar, although some slight ringing occurs at the end of the CDM event that results in some negative-going peaks.

With a 400 V charging voltage, a socketed CDM discharge will have a peak current of 2.1 A. However, the very short duration of the overall CDM event results in an overall discharge of relatively low energy.

**Summary of ESD Models**

Table I is a reference table that compares the most important characteristics of the three ESD simulation models.

**Table I.**

Model	HBM	MM	Socketed CDM
Simulate	Human Body	Machine	Charged Device
Origin	US Military Late 1960s	Japan 1976	AT&T 1974
Real World	Yes	Generally No	Yes
RC	1.5 kΩ, 100 pF	0 Ω, 200 pF	1 Ω, 1 pF-20 pF
Rise Time	<10 ns	14 ns*	400ps**
I <sub>PEAK</sub> at 400 V	0.27 A	5.8A*	2.1A**
Package Dependent	No	No	Yes
Leakage Recovery	No	No	Yes
Standard	MIL-STD-883 Method 3015	ESD Assoc. Standard S5.2; EIAJ Standard ED-4701, Method C-111	ESD Assoc. Draft Standard DS5.3

\* These values are per ESD Association Standard S5.2. EIAJs standard ED-4701 Method C-111 includes no waveform specifications.

\*\* These values are for the direct charging (socketed) method.

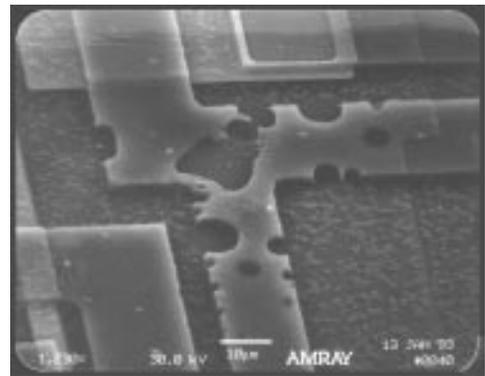
**Prevention**

When auditing a facility in which ESD protective measures will be taken, the following should be considered: <sup>4</sup>

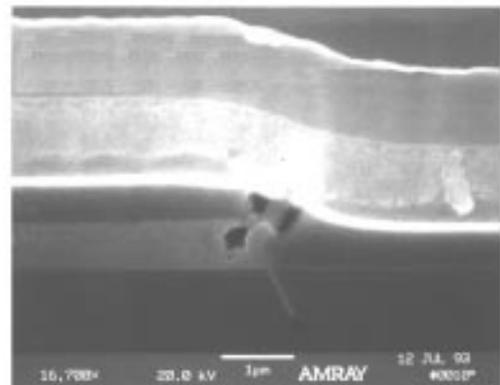
- There must be a grounded workbench on which to handle static sensitive devices incorporating:
  - a) Personal ground strap (wrist strap)
  - b) Conductive trays or shunts, etc.
  - c) Conductive work surface
  - d) Conductive floor or mat
  - e) A common ground point
- All steel shelving or cabinets used to store devices must be grounded.
- The relative humidity should be controlled; the desirable range is 40 to 60 percent. Where high relative humidity levels cannot be maintained, the use of ionized air should be used to dissipate electrostatic charges.
- All electrical equipment used in the area must be grounded.

- Prohibit the use of prime static generators, e.g., Scotch tape.
- Follow up with ESD audits at a minimum of three month intervals.
- Training: Keep in mind, the key to an effective ESD control program is "TRAINING." Training should be given to all personnel who come in contact with integrated circuits and should be documented for certification purposes, e.g., ISO 9000 audits.

Determining whether a device failed as a result of ESD or Electrical Overstress (EOS) can be difficult and is often best left to Failure Analysis Engineers. Typically ESD damage is less obvious than that of EOS when electrical analysis and internal visual analysis are performed. In the case of ESD, events of 1 kV or more (depending on the ESD rating of the device) can rupture oxides (inter layer dielectric of the die) and damage junctions in less than 10 ns (see Figure 6). Alternately, EOS conditions leading to 1 to 3 amps of current for a duration of ≥1 ms can cause sufficient self-heating of bond wires to fuse them. Such conditions can occur as a result of latch-up. Lower currents can cause rapid melting of chip metallization and other interconnect layers (see Figure 5).



*Figure 5. Scanning Electron Microscope View of a Fused Metallization Site, as a Result of Electrical Overstress*



*Figure 6. Scanning Electron Microscope Cross-Sectional View of a CDM ESD Site. This subsurface site could not be viewed from the surface with an optical microscope.*

A quick analysis can be performed on site to evaluate if a device may have been overstressed or may have been subjected to an ESD event. In order to perform this analysis, to compare the pin-to-pin I/V results of the suspect device to those of a known good device, a curve tracer or similar equipment should be used. A typical set of I/V traces for a short circuit, open circuit or ESD leakage on a digital input pin (with reference to the  $V_{SS}$  supply pin) of a 12-bit DAC is shown in Figure 7.

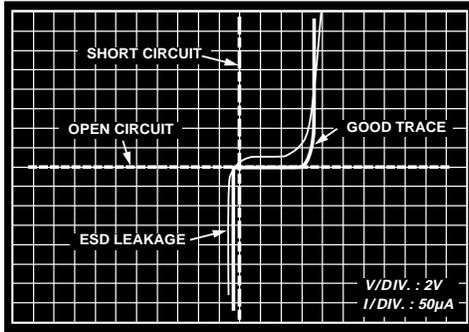


Figure 7. Example of an Unpowered Curve Trace Analysis of a Digital Pin versus a Supply Pin ( $V_{SS}$ )

### LATCH-UP

Latch-up is a potentially destructive situation in which a parasitic active device is triggered, shorting the positive and negative supplies together. If current flow is not limited, electrical overstress will occur. The classic case of latch-up occurs in CMOS output devices, in which the driver transistors and wells form a *pnpn* SCR structure when one of the two parasitic base-emitter junctions is momentarily forward biased during an overvoltage event. The SCR turns on and essentially causes a short between  $V_{DD}$  and ground.

### Triggering Mechanisms

There are two main triggering mechanisms. *First*, if the input/output (I/O) pin voltage is raised above the positive supply, or lowered below the negative supply, one of the parasitic transistors is turned on. The current returning to the supply through the collector causes a voltage drop across the base-emitter of the second parasitic transistor. In turn, the collector current of the second transistor maintains a forward bias on the base-emitter of the first transistor. If the product of the two transistor gains is greater than unity, the condition may be self-sustaining and can persist even after the external voltage is removed.

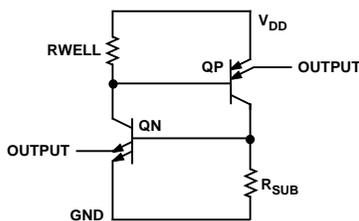


Figure 8. Parasitic SCR. The Diffusions in a CMOS output form a parasitic SCR. The resistors are labeled for an n-well process.

This triggering mechanism can occur if excessive voltage overshoot is present at the I/O pin, or if the signal arrives at the input before the power supplies are applied to the device, or due to electrostatic discharge. This latch-up is usually limited to the devices directly connected to the pin.

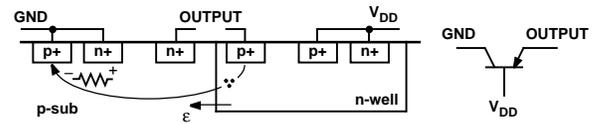


Figure 9a. Output Overvoltage Triggering. Initial hole current flows when the output voltage is raised above  $V_{DD}$ . This current causes a voltage rise in the substrate under the NMOS device.

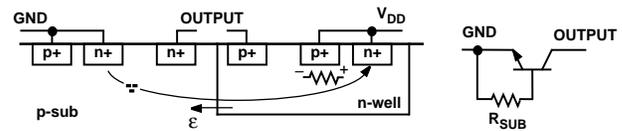


Figure 9b. Current Multiplication. The substrate voltage rise actively biases the second parasitic transistor into conduction. The electron current subsequently causes a voltage drop in the n-well, further turning on the first transistor. If the product of the current gains is larger than one, the final current flow between the supplies can be self-sustaining, limited only by internal resistance's, i.e., an SCR.

Although triggering is by an overvoltage event (typically of only a diode drop above or below the power supplies), the industry practice is to classify the I/O susceptibility in terms of the amount of excess current the pin can source or sink in this overvoltage condition before the internal parasitic resistance's develop enough voltage drop to sustain the latch-up condition. A value of 100 mA is generally considered adequate, with 200 mA considered immune to latch-up.

The *second* triggering mechanism occurs if a supply voltage is raised enough to break down an internal junction, injecting current into the SCR previously described.

This triggering mechanism can occur due to supply transients, or electrostatic discharges shunted to a supply rail. Unlike the case of I/O triggering, latch-up can occur anywhere on the die and is not limited to the vicinity of the external power connections or I/O pins.

The susceptibility to power supply overvoltage is usually limited by the fabrication process on which the device is manufactured, and can be found in the data sheet under the Absolute Maximum Rating specification. If this rating is exceeded, permanent EOS damage may occur. Operating a device near the maximum ratings may degrade the long term reliability of the device. Also the electrical specifications are applicable only at the supply specified on the data sheet and will not be guaranteed above these ratings.

## Design Rules

The following is a set of rules to be followed for all designers using CMOS and Bipolar-CMOS ICs: <sup>5</sup>

1. Digital inputs and outputs should not be allowed to exceed  $V_{DD}$  by more than 0.3 volts at any time. This includes a power-down situation when  $V_{DD} = 0$  volts.
2. Digital inputs and outputs should also not be allowed to go below DGND by more than  $-0.3$  volts.
3. For mixed signal devices, DGND should not be allowed to exceed AGND by 0.3 volts.
4. For a CMOS or Bipolar-CMOS DAC,  $I_{OUT}$  should, in general, not be allowed to drop below AGND by more than 0.3 volts. Some DACs can tolerate significant  $I_{OUT}$  current flow, however, without any danger of latch-up.

## Latch-Up Prevention Techniques

The following recommendations should be implemented in general, for all applications with CMOS and Bipolar-CMOS ICs that violate one or more of the previously discussed rules:

1. If the digital inputs or outputs of a device can go beyond  $V_{DD}$  at any time, a diode (such as a 1N914) connected in series with  $V_{DD}$  will prevent SCR action and subsequent latch-up. This works because the diode prevents the base current of the parasitic lateral-PNP transistor from flowing out the  $V_{DD}$  pin, thus preventing SCR triggering. This is shown in Figure 10.

Diodes are also a reliable solution if power-up sequencing is identified as the failure mechanism. In such a case, the insertion of a Schottky diode between the logic inputs and the  $V_{DD}$  supply rail (the anode of the diode connected to the logic inputs), will ensure that the logic inputs do not exceed the  $V_{DD}$  supply by more than 0.3 volts, thus preventing latch-up of the device.

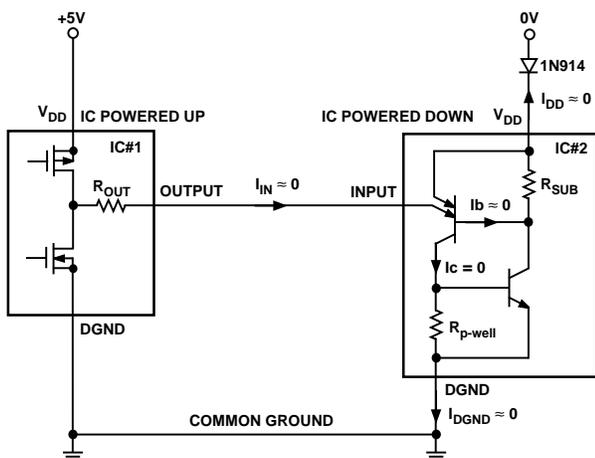


Figure 10. Adding an inexpensive silicon diode in series with the  $V_{DD}$  pin of the unpowered IC effectively prevents the parasitic lateral-PNP transistor's base current from flowing and inhibits SCR action.

However, the one *exception* to this rule is when the input range of a device exceeds the supply voltage range of the device, e.g., by design the AD7893-10 12-bit A/D subsystem, the input range is  $\pm 10$  V and the supply is +5 V.

2. If the digital inputs and outputs of a device can go below DGND at any time, a Schottky diode (such as an HP5082-2835) connected from those inputs or outputs to DGND will effectively clamp negative excursions at  $-0.3$  volts to  $-0.4$  volts. This prevents the emitter-base junction of the parasitic NPN transistor from being turned on, and also prevents SCR triggering. Figure 11 shows the connections for the Schottky diodes.

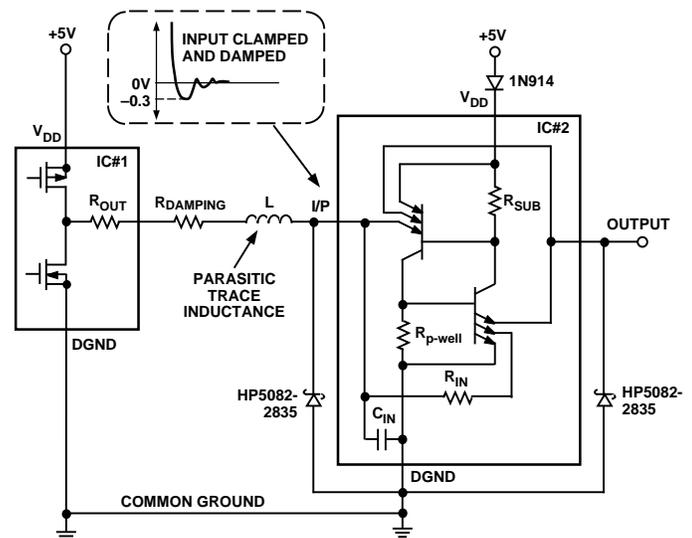


Figure 11. Adding Schottky diodes from the inputs and outputs of a CMOS IC to DGND protects against undervoltages causing conduction of the parasitic NPN, thus inhibiting SCR action. The series damping resistor makes ringing due to long PC board traces die out more quickly.

3. If the DGND potential can occasionally exceed AGND by more than 0.3 volts, a Schottky diode placed between the two pins of the device will prevent conduction of the associated parasitic NPN transistor. This provides additional protection against latch-up as shown in Figure 12. An extra diode connected in inverse parallel with the one just mentioned provides clamping of DGND to AGND in the other direction and will help to minimize digital noise from being injected into the IC.

To identify over- and under-voltage events as described in points (2) and (3) above, the use of a storage oscilloscope is suggested, set at the maximum ratings specification for each pin. Set the Time/Div. to the minimum setting on the oscilloscope (preferably in the ns range). This test should be conducted over a long period of time, e.g., overnight.

4. In circuits where the  $I_{OUT}$  pin of a CMOS IC can be pulled below AGND, another Schottky diode clamp between these two terminals will prevent sensitive

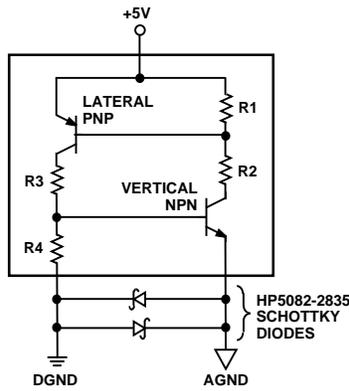


Figure 12. Connecting Schottky diodes between DGND and AGND prevents conduction of the parasitic NPN transistor, and helps to minimize injected noise from DGND to the analog output.

ICs from latching up. This condition sometimes occurs with high speed bipolar operational amplifiers that are used as current-to-voltage converters following a DAC. During power-up or power-down transitions, the op amp's inverting input presents a low impedance from I<sub>OUT</sub> to the negative supply rail. An unprotected DAC may fail without the recommended Schottky diode clamp to AGND.

- In designs that have long digital PC board traces between components and are therefore prone to inductive ringing problems, a series damping resistor of 10 Ω–100 Ω will be beneficial. This resistor increases the damping factor of the equivalent series RLC network and causes the ringing to decay more quickly. This will help to prevent conduction of the input or output protection diodes.

### High Voltage Transients

If power supply overvoltage is identified as the failure mechanism, a reliable solution is the insertion of a TransZorb\* transient voltage suppressor (TVS). What is a TVS and how does it work?

Transient voltage suppressors<sup>6</sup> (TVSs) are devices used to protect vulnerable circuits from electrical overstress such as that caused by ESD, inductive load switching and lightning-induced line transients. Within the TVS, damaging voltage spikes are limited by clamping or avalanche action of a rugged silicon pn junction which reduces the amplitude of the transient to a nondestructive level.

In a circuit, the TVS should be “invisible” until a transient appears. Electrical parameters such as breakdown voltage ( $V_{BR}$ ), standby (leakage) current ( $I_D$ ), and capacitance should have no effect on normal circuit performance.

To limit standby current and to allow for variations in  $V_{BR}$  caused by the temperature coefficient of the TVS, the TVS breakdown voltage is usually 10% above the

reverse standoff voltage ( $V_R$ ), which approximates the circuit absolute maximum operating voltage. When a transient occurs, the TVS clamps instantly to limit the spike voltage to a safe level, called the clamping voltage ( $V_C$ ), while conducting potentially damaging current away from the protected component.

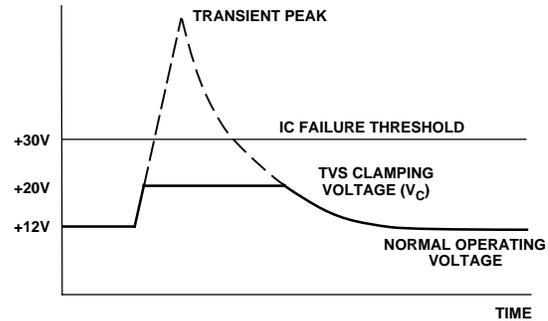


Figure 13. Transients of several thousand volts can be clamped to a safe level by the TVS.

TVSs are designed, specified and tested for transient voltage protection, while a Zener diode is designed and specified for voltage regulation. Therefore, for transient protection the TVS should be selected over the Zener.

The surge power and surge current capability of the TVS are proportional to its junction area. Surge ratings for silicon TVS families are normally specified in kilowatts of peak pulse power ( $P_P$ ) during a given waveform. Early devices were specified with a 10/1000 μs waveform (10 μs rise to peak and 1000 μs exponential decay to one half peak), while more recent devices are rated for an 8/20 μs test waveform. Power ratings range from 5 kW for 10/1000 μs, down to 400 W for 8/20 μs. This power is derived from the product of the peak voltage across the TVS and the peak current conducted through the device.

TVSs have circuit operating voltages available in increments from 5 V up to 376 V for some families. Because of the broad range of voltages and power ratings available (as well as the universal presence of transient voltages), TVSs are used in a wide variety of circuits and applications.

As an example, consider a pressure transducer which operates at 28 V, placed in an environment in which it encounters a transient voltage of 140 V peak, having a source impedance of 2 Ω and a duration of 10/1000 μs. The failure threshold of the transducer is 40 V, therefore the TVS must clamp at 40 V or less. The current delivered by this transient is:

$$I = (140 \text{ V} - 40 \text{ V}) / 2 \Omega = 50 \text{ A}$$

Note that the voltage clamping action of the TVS results in a voltage divider whereby the open circuit voltage of the transient appears across the combination of the source impedance and the TVS device. Thus the TVS

\*TransZorb is a registered trademark of General Semiconductor Industries, Inc.

clamping voltage is subtracted from the transient voltage leaving a net source voltage of 100 V. When the clamping voltage is high compared to the transient peak voltage, the current is significantly reduced.

This circuit can be protected with a 5 kW rated TransZorb TVS which will easily sustain the surge current.

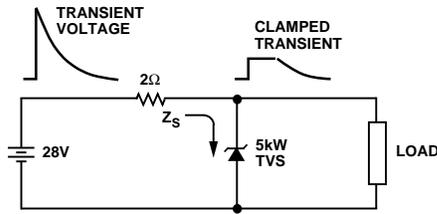


Figure 14. A 5 kW TVS is required to handle the surge current.

An alternate and more economical approach is to add a series resistor to effectively increase the source impedance thus limiting surge current as illustrated in Figure 15. Since the current drawn by the transducer under normal operation is small (<20 mA typical), performance is not adversely affected by a reduction in supply current.

For a small load current, 10 mA, the voltage drop across the added resistance is minimal, about 250 mV for a 25 ohm resistor. Adding this resistor reduces the surge current to:

$$I = (140 V - 40 V) / (2 \Omega + 25 \Omega) = 3.7 A$$

This is less than one-tenth the surge current without the resistor. A TVS with lower power rating is able to handle the resulting current. In this case a 500 W suppressor replaces the 5 kW device, saving board space and cost.

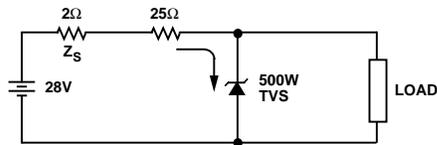


Figure 15. The series resistor reduces transient current allowing a much smaller TVS to be used.

Carbon composition resistors are recommended for this application because of their energy dissipation capability. Steady state power dissipated by the resistor ( $V \times I$ ) is 2.5 mW requiring the lowest rated resistor available for adequate margin.

## TYPICAL TVS APPLICATIONS

### DC Line Applications

TransZorb TVSs on power lines prevent IC failures caused by transients, power supply reversals or during switching of the power supply between on and off (Figure 16).

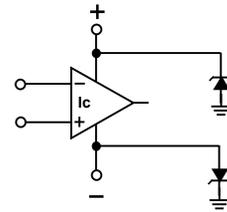


Figure 16.

For power sources utilizing the TransZorb TVS, the TransZorb TVS is chosen such that the reverse stand-off voltage is equal to or greater than the dc output voltage. For certain applications it may be more desirable to replace the series resistor (R) with an inductor (Figure 17).

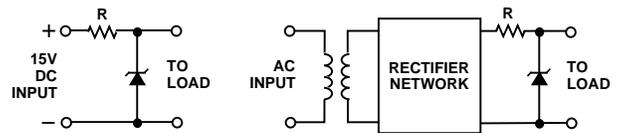


Figure 17.

### Signal Line Applications

Input pins are vulnerable to low energy, high voltage static discharges or crosstalk transmitted to the signal wires. Limited protection is provided by the clamp diode or an input network within the IC substrate (Figure 18).

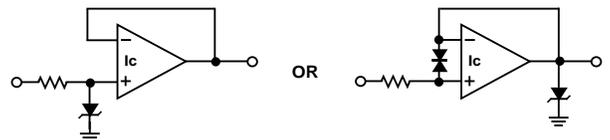


Figure 18.

Transients generated on the line can vary from a few microseconds to several milliseconds in duration and up to 10,000 volts in magnitude. Excess current passing through the diode can cause an open circuit condition or a slow degradation of the circuit performance. TransZorb TVSs located on the signal line can absorb this excess energy (Figure 19).



Figure 19.

A further reference on the subject of using TransZorbs for circuit protection is Analog Devices Application Note AN-311, entitled "How to Reliably Protect CMOS Circuits against Power Supply Overvoluting."

## IN SUMMARY

Designing an application with maximum protection of the integrated circuits is a challenging problem with a solution that depends on many factors. The following is a brief summary of the protection schemes discussed in this application note:

1. Personnel should be trained in the proper handling techniques for prevention of EOS/ESD damage.
2. A good facilities ground system including shielding of equipment and data lines should be implemented.
3. Use transient suppressors judiciously, i.e., check if there are spikes on the supply and the ground lines which may exceed the maximum ratings of those pins.
4. Review the proper power-up sequence of the device(s). The correct order should normally be: GND, Main supplies (if possible the substrate supply being first),  $V_{CC}$ ,  $V_{REF+/-}$  and finally all other pins.
5. Review the data sheet, in particular the maximum ratings section.

Remaining devices from a lot that may have been mistested or subjected to the same conditions as those of any failing devices should be evaluated to determine if latent damage may be present. This analysis should be performed due to the possibility that overstress conditions existed which did not cause immediate failure but induced subtle damage that could result in long-term reliability problems.

Finally, the issue of input overvoltage protection for amplifiers is not discussed in this application note. However, it is exclusively discussed in two other Analog Devices publications; (1) Joe Buxton, "Simple Techniques Protect Amplifiers from Input Overvoltage," *Analog Dialogue* 28-3, 1994, and (2) Joe Buxton, "Input Overvoltage Protection," *System Applications Guide*, Analog Devices, 1993, pp 1-56 to 1-74.

## REFERENCES

- <sup>1</sup>Henry Domingos, "Circuit Design for EOS/ESD Protection," Proc. 1982 EOS/ESD Symp., pp. 1-17 to 1-21.
  - <sup>2</sup>John A. Schmidt, Manager of Technical Services IMCS Corporation, Santa Clara, CA, "CDM-The Newest ESD Test Model," 1991.
  - <sup>3</sup>MIL-STD-883 Method 3015, "Electrostatic Discharge Sensitivity Classification," Military Standard Test Methods and Procedures for Microelectronics.
  - <sup>4</sup>*ESD Prevention Manual*, 1986. Norwood MA; Analog Devices Inc., pp 9-11. Contains additional references.
  - <sup>5</sup>Mark Alexander, "Understanding and Preventing Latch-Up in CMOS DACs," AN-109. Free from Analog Devices, PMI Division.
  - <sup>6</sup>*General Instrument, Power Semiconductor Division Data Book/11th edition*, pp. 633, 696-703. Contains additional references.
- Andrew Olney, Analog Devices, Inc., personal communication